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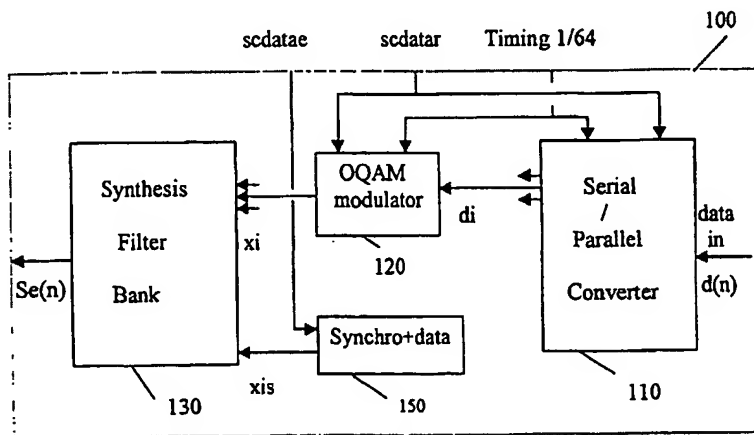
(43) International Publication Date
17 May 2001 (17.05.2001)

PCT

(10) International Publication Number
WO 01/35561 A1

- (51) International Patent Classification⁷: H04J 1/20, H04L 7/00, 27/01, 27/34 (74) Agent: SCHREIBER, Donald, E.; P.O. Box 64150, Sunnyvale, CA 94088-4150 (US).
- (21) International Application Number: PCT/US00/42048 (81) Designated States (*national*): JP, US.
- (22) International Filing Date: 9 November 2000 (09.11.2000) (84) Designated States (*regional*): European patent (AT, BE, CH, CY, DE, DK, ES, FI, FR, GB, GR, IE, IT, LU, MC, NL, PT, SE, TR).
- (25) Filing Language: English
- (26) Publication Language: English
- (30) Priority Data: 99/14036 9 November 1999 (09.11.1999) FR
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- Published:
— With international search report.
— Before the expiration of the time limit for amending the claims and to be republished in the event of receipt of amendments.
- For two-letter codes and other abbreviations, refer to the "Guidance Notes on Codes and Abbreviations" appearing at the beginning of each regular issue of the PCT Gazette.

(54) Title: MULTICARRIER DIGITAL TRANSMISSION SYSTEM USING AN OQAM TRANSMULTIPLEXER



Digital Multicarrier Emitter

(57) Abstract: An emitter converts a serial input data stream into a set of parallel substreams. An OQAM modulator (120) receives and supplies each substream to an input of a synthesis filter bank (130). Synchronization input(s) of the filter bank receive an OQAM signal that carries a data sequence. This sequence contains frame, superframe and hyperframe synchronization patterns, and specifies the number of bits allocated to each subchannel. A receiver (200) includes an analysis filter bank (210) that decomposes the multicarrier signal into a set of elementary signals for each subchannel. A synchronizing processing block (270) receives output(s) of the filter bank for synchronization subchannel(s). The block (270) includes a first cascade of blocks that control receiver sampling times, and a second cascade of blocks that extract synchronization patterns and subchannel bit assignment data. Other filter bank outputs are each coupled to a cascade subchannel equalizer (220) followed by a data extractor (230) and a parallel-to-serial converter (240).

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**Multicarrier Digital Transmission System
Using an OQAM Transmultiplexer**

Technical Field

5 The present invention relates to systems for the transmission of digital data over a communication channel using a multicarrier modulation and, more particularly, to an improved OQAM transmultiplexer method for use in such systems.

10 Background Art

 A multicarrier transmission system, as opposed to a single carrier system, uses a set of different frequencies distributed in the transmission channel frequency band to carry the data. The main advantage is that the bit rate can be adjusted for each
15 carrier, according to the noise and distortion power in the vicinity of this carrier. Thus, a better approximation of the theoretical information capacity limit can be expected and, particularly, poor quality channels can be exploited, like some wireless communication channels, power lines or the telephone
20 subscriber lines at high or very high frequencies. A detailed description of existing multicarrier transmission systems and their merits compared to single carrier systems is given in the book by W.Y.Chen: « DSL-Simulation Techniques and Standards Development for Digital Subscriber Line Systems », MacMillan
25 Technical Publishing, Indianapolis, USA, 1998.

 In order to efficiently perform multicarrier transmission, two basic approaches have been considered so far. The first one and most widely used is called OFDM (Orthogonal Frequency Division Multiplexing) or DMT (Digital Multi-Tone) and it is
30 based on the FFT (Fast Fourier Transform). It has been a subject of intense research and development efforts. In that scheme, the data are arranged in blocks which are transmitted by orthogonal carriers, and separated by guard times, which have to be greater than the channel impulse response, to preserve the orthogonality
35 of the carriers at the receiving side. In spite of the potential of the approach, OFDM/DMT suffers from a number of weaknesses, which, overall, make it perform hardly better than single carrier transmission: a complex time equalizer has to be introduced in

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front of the receiver to reduce the channel impulse response length, very precise time synchronization is necessary, a long initialization phase is required, and the carriers, and subchannels, are poorly separated, which reduces the capacity of the system in the presence of jammers. In fact, a good quality channel is necessary for that scheme to work properly. Ample documentation can be found in the literature and a good list of references is given in the book by W.Y.Chen.

A second approach aims at overcoming some of the OFDM/DMT limitations through the use of more sophisticated transforms than the FFT, namely, lapped transforms and wavelet transforms. The idea is to improve the separation between carriers, or subchannels. A lot of theoretical work has been done about this subject, see for example the paper by S.D.Sandberg and M.A.Tzannes: « Overlapped Discrete Multitone Modulation for High Speed Copper Wire Communications », IEEE-JSAC, Vol.13, N°9, Dec. 1995. Although they improve the subchannel separation, the lapped and wavelet approaches still retain some of the crucial OFDM/DMT limitations and particularly the time synchronization requirements.

In fact, the ideal approach for multicarrier transmission is one in which the subchannels are made independent and this is achieved by filter banks. This has been recognized a long time, and an efficient implementation of filter banks for transmission systems, based on the combination of an FFT processor with a polyphase network, has been presented in the paper by M.Bellanger and J.Daguet: « TDM-FDM Transmultiplexer: Digital Polyphase and FFT », IEEE Transactions on Communications, Vol.COM-22, Sept.1974. Later on, a technique called OQAM (Orthogonal Quadrature Amplitude Modulation) has been proposed for multicarrier transmission with filter banks, see the paper by B.Hirosaki, « An Orthogonally Multiplexed QAM System Using the Discrete Fourier Transform », IEEE Trans. on Communications, Vol.COM-29, July 1981. Its main feature is that the subchannel sampling rate is twice the Nyquist subchannel frequency, or subchannel spacing, and the data are transmitted alternatively on the real and the imaginary part of the complex signal in any subchannel, with, again, an alternation between two adjacent

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subchannels. With this technique, intersymbol interference is eliminated in a subchannel and between adjacent subchannels. The distortions introduced by the transmission channel can be eliminated by a multibranch equalizer in each subchannel.

5 Recently, it has been shown that a single branch equalizer can be used, see the paper by L.Qin and M.Bellanger, « Equalization issues in Multicarrier Transmission Using Filter Banks », Annals of Telecommunications, Vol.52, N°1-2, January 1997.

10 In spite of its potential theoretical advantages, the OQAM multicarrier approach is seldom considered for implementation in practical systems. A key reason is that the real/imaginary alternation principle raises problems, which have not been adequately solved thus far, for the equalization algorithms, the carrier synchronization and the system timing organization.

15

Disclosure of Invention

It is a primary object of the present invention, to achieve a highly robust and efficient multicarrier transmission system, using the transmultiplexer concept of filter banks in combination
20 with OQAM modulation.

The above and other objects are achieved in accordance with the present invention wherein a signal containing synchronization patterns which define a timing structure consisting of frames, superframes and hyperframes is fed, in the emitter, to the input
25 of one or several subchannels reserved for synchronization, the relevant information being carried by the magnitude or envelop of the complex OQAM signal. The same signal also contains service data giving the number of bits allocated to each subchannel. In the other subchannels, a short fixed pattern is
30 introduced periodically to serve as a reference signal for the subchannel equalizers in the receiver.

At the output of the analysis filter bank in the receiver, the signal corresponding to the synchronization subchannel(s) is coupled to a first cascade containing an amplitude equalizer, an
35 envelop detector and a filter that delivers the control signal for the phase lock loop associated with the receiver clock generator and to a second cascade containing an amplitude and phase equalizer, a data detector and a block for the identifica-

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tion of the superframe and hyperframe synchronization patterns and the service data extraction. The other outputs of the analysis filter bank are coupled to cascade subchannel equalizers consisting of three elements each, namely an amplitude equalizer, 5 a phase equalizer and a fine equalizer. Every subchannel equalizer is followed by a data extractor and both use the information provided by the synchronization subchannel to complete their functions. The output error signals are used to determine the number of bits assigned to each subchannel and the 10 information is transmitted to the distant terminal via the synchronization subchannel(s) every hyperframe.

With the system of the invention, no initialization specific sequence is necessary at the beginning of a transmission session or after an interruption, and the bit rate distribution among the 15 subchannels can be adjusted continuously in time during the transmission.

These and other features, objects and advantages will be understood or apparent to those of ordinary skill in the art from the following detailed description of the preferred embodiment 20 as illustrated in the various drawing figures.

Brief Description of Drawings

The invention will be more fully appreciated from the following detailed description when the same is considered in 25 connection with the accompanying drawings, in which:

FIG. 1 is a simplified schematic block diagram of a multicarrier transmission system, in accordance with the present invention;

FIG. 2 is a schematic block diagram of the digital 30 multicarrier emitter;

FIG. 3 is a drawing showing the waveform of the envelop of the signal in the synchronization subchannel;

FIG. 4 is a schematic block diagram of the digital multicarrier receiver;

35 FIG. 5 is a schematic block diagram of the subchannel equalizer; and

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FIG. 6 is a schematic block diagram showing the functions involved in the processing of the signals received in the synchronization channel.

5 Best Mode for Carrying Out the Invention

The block diagram of a multicarrier transmission system is shown in FIG. 1, for the case of a digital subscriber telephone line application. The input data stream $d(n)$ is fed to a multicarrier emitter 100, which forms the signal $Se(n)$ and is
10 itself coupled to a module 10 that performs the digital-to-analog (D/A) conversion and the emitter analog front end functions. Basically, the emitter analog front end consists of an amplifier and a low-pass or pass-band filter to limit the spectrum sent to the hybrid circuit 11. The hybrid is connected to the twisted
15 pair line 14 and its receiving port is connected to a module 12 that performs the receiver analog front end functions and the analog-to-digital (A/D) conversion. The receiver analog front end consists of a low-pass or band-pass filter to prevent aliasing and a variable gain amplifier. If symmetric, or full
20 duplex transmission is contemplated, the A/D converter is coupled to an echo canceller 13 that ensures an adequate level of separation between the two directions of transmission. The echo canceller produces the signal $Sr(n)$ and it is coupled to a multicarrier receiver 200 that delivers the output data stream
25 $d'(n)$. A detailed description of the analog front ends, hybrid circuits, A/D and D/A converters as well as echo cancellers is given in W.Y.Chen's book.

The present invention is concerned with the multicarrier emitter block 100 and receiver block 200 shown in greater details
30 in FIGs. 2 and 4 respectively.

Turning to FIG. 2, the input data $d(n)$ are processed by a cascade of three blocks, namely a serial/parallel converter 110, an OQAM modulator 120 and a synthesis filter bank (SFB) 130, to produce the emitted digital multicarrier signal $Se(n)$. Conversely,
35 ly, as shown in FIG. 4, the received multicarrier digital signal $Sr(n)$ is processed by a cascade of 4 blocks, namely an analysis filter bank (AFB) 210, a subchannel equalizer 220, a data extractor 230 and a parallel/serial converter 240, to produce the

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output data sequence $d'(n)$. In the absence of transmission errors, $d'(n)$ and $d(n)$ are identical, except for a delay.

The filter banks, SFB 130 and AFB 210 consist of an FFT processor, coupled to a polyphase network as described in the paper by M.Bellanger and J.Daguet. Denoting by f_s the sampling frequency of the multicarrier signal and by N the size of the FFT, which is twice the number of real subchannels, the subchannel frequency spacing is f_s/N and the SFB and AFB operate at the rate $2(f_s/N)$. For example, in subscriber line transmission, the following values may be selected: $f_s = 2048$ kHz; $N = 512$; $2(f_s/N) = 8$ kHz.

The specificity of the filter banks, SFB 130 and AFB 210 resides in the values of their coefficients, that are the same for both, or very close. The filter bank coefficients are computed from a prototype filter frequency response $H(f)$ that is half-Nyquist in the pass-band and provides the maximum attenuation in the stop-band. Therefore, the cascade of the filter banks SFB and AFB exhibits a frequency response $H^2(f)$ that satisfies the first Nyquist criterion. It is advantageous to have $H^2(f)$ satisfy also the second Nyquist criterion, because intermediate signal samples take on well defined values. For example, if the data samples fed to the real or imaginary part of a subchannel are ± 1 , the intermediate signal samples at the output of the SFB-AFB cascade are $\{ +1; 0; -1 \}$.

A possible choice for the prototype filter frequency response is an approximation of the following function

$$\begin{aligned} H_t(f) &= \cos(\pi N f / 2 f_s) & ; & \quad 0 \leq |f| \leq f_s / N \\ H_t(f) &= 0 & ; & \quad f_s / N \leq |f| \leq f_s / 2 \end{aligned} \quad (1)$$

using the Fourier series expansion. Accordingly, a prototype filter with $M=2P+1$ coefficients has the following coefficient values, in the above example.

$$h_i = \frac{\cos(\pi i / 256)}{1 - (i / 128)^2} \quad ; \quad -P \leq i \leq P \quad (2)$$

The input signal x_i to the SFB block 130 that corresponds to subchannel i , is supplied by the OQAM modulator 120, a device that associates the input data d_i to quantized signal samples x_i according to predetermined rules, as is well known in data transmission and described for example in the book by W.Y.Chen.

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The specificity here is that the signal samples take on real and imaginary values alternatively to obey the OQAM principle and the number of levels is determined by an external control signal denoted « scdatar » in FIG. 2. The control signal scdatar
5 adjusts the number of bits transmitted by a subchannel to its estimated capacity, as will be explained below. For example, if 1 bit can be carried by subchannel i , the sample x_i may take on the following values: ± 1 . But, if 2 bits can be carried, then the sample x_i may take on the values: -1.5 ; -0.5 ; $+0.5$; $+1.5$.

10 The serial-to-parallel converter 110 splits the input bit stream $d(n)$ into as many substreams as used subchannels and, for each substream, constitutes groups of bits d_i , under the control of the external signal scdatar, to feed the OQAM modulator 120. An additional external signal, denoted « timing $1/64$ » in FIG.
15 2, is used to insert a reference pattern in the signal sequence as will be explained below and it is fed to both blocks serial/parallel converter and OQAM modulator.

In the system, at least one subchannel is used to carry a synchronization signal described hereafter and service data. The
20 corresponding signal x_{is} is generated by the « synchro+data » unit 150, the service data, denoted « scdatae » in FIG. 2, being supplied by the receiver 200 shown in FIG. 4.

The timing of the system is organized in 3 levels which will be referred to as follows.

- 25 1) **frame**: it is the basic period in the system, associated with the subchannel spacing f_s/N . For example, if $f_s/N = 4$ kHz, a frame is 0.25 ms. The frame is used for payload transmission, amplitude subchannel equalization and
30 synchronization.
- 2) **superframe**: a duration of N_1 frames. For example, if $N_1 = 64$ the superframe length is 16 ms. It is used for supervised subchannel equalization, noise level measurement and synchronization.
- 35 3) **hyperframe**: a duration of N_2 superframes. For example, if $N_2 = 64$ the hyperframe length is 1024 ms. It is used to confirm or modify the bit assignments in the subchannels.

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Turning to synchronization, at least one subchannel is used to transmit a specific signal. For example, it can be subchannel 69, whose central frequency is $4 \text{ kHz} \times 69 = 276 \text{ kHz}$. The specific synchronization signal is designed to provide an efficient and robust control of the sampling times in the receiver and perform frame, superframe and hyperframe alignment. It contains the following superframe synchronization pattern.

$$\text{SFP} = \{ | | | - | - | - | | | | - | - | - | | \}$$

With the real and imaginary alternation required by the OQAM technique, and the filtering operation performed by the filter banks, such a pattern produces, at the receiving end and in the absence of amplitude distortion in the transmission channel and no signal present in the neighboring subchannels, a complex signal whose squared magnitude $v(n)$ is a $f_s/2N$ frequency sinewave of amplitude 0.5, added to a zero-frequency component of amplitude 1.5, as shown in FIG. 3. With the numerical values given as example, $f_s/2N = 2 \text{ kHz}$, SFP has a duration of 2 ms and produces 4 periods of the 2 kHz sinewave, as is clearly apparent in the left part of FIG. 3. Since the superframe has a length of 16 ms, 14 ms are available for the transmission of service data. These data are encoded as

$$P0 = \pm \{ | - | - | | \} \text{ for a « zero » ; } P1 = \pm \{ | | | | \} \text{ for a « one »}$$

Two consecutive data are separated by a period of the 2 kHz sinewave, as shown in FIG. 3.

The signal used to control the phase lock loop associated with the oscillator that delivers the received signal sampling frequency, or receiver clock generator, is obtained by filtering the 2 kHz component in $v(n)$. This function is advantageously realized in two steps, as follows. A signal $c(4n)$, with sampling frequency 2 kHz, is obtained by

$$c(4n) = v(4n) - v(4n-1) - [v(4n-2) - v(4n-3)] \quad (3)$$

Then, an averaging operation is performed to attenuate the noise and the interferences from the neighboring subchannels

$$ca(4n) = (1-\epsilon) ca[4(n-1)] + \epsilon c(4n) \quad (4)$$

where ϵ is a small constant, for example $\epsilon = 10^{-3}$. The signal $ca(4n)$ is used to control the phase lock loop of the clock generator.

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The sign \pm in P0 and P1 is used as shown in FIG. 3 to ensure that rising and falling edges of the 2 kHz signal keep a fixed relative position in time, regardless of the transmitted service data.

5 The hyperframe synchronization pattern HFP occurs every 64 superframes and it consists of a superframe in which the pattern SFP is repeated 4 times: $HFP = \{SFP, SFP, SFP, SFP\}$.

In view of equalization in the receiver, an additional feature of the OQAM modulation block 120 in the emitter, is that
10 it imposes fixed values to the first two samples of the superframe in each subchannel, for example: $\pm [1; 1]$. A specific sign may be attributed to each subchannel, in order to avoid producing a large peak in the emitted multicarrier signal $Se(n)$ at the beginning of each superframe.

15 In the receiver, the multicarrier received signal $Sr(n)$ is processed by a cascade of 4 blocks, namely the analysis filter bank 210, a subchannel equalizer 220, a data extraction module 230 and a parallel-to-serial converter 240. The subchannel equalizer 220, which consists of a cascade of 3 distinct
20 equalizers, is shown in more details in FIG. 5.

Turning to FIG. 5, in subchannel i , the amplitude equalizer 221 receives the input sequence $xir(n)$ and a reference amplitude ra supplied by the bit assignment module 250. This reference amplitude ra represents the theoretical value of the root mean
25 square of the power of the data signal in the subchannel. For 1-bit data, $ra=1$. The amplitude equalizer 221 computes a variable gain $gl(n)$, multiplies the input signal by that gain and transfers the result $yi(n)$ to the phase equalizer 222. The variable gain is obtained through the two following operations

$$30 \quad sgm(n+1) = (1-\epsilon) sgm(n) + \epsilon |xir(n+1)| \quad (5)$$

where $|x|$ stands for the modulus of x and ϵ is a small real number, for example $\epsilon = 10^{-3}$.

$$gl(n+1) = ra / sgm(n+1) \quad (6)$$

Next, the phase equalizer 222 multiplies its complex input signal
35 $yi(n) = yir(n) + j yii(n)$ by a complex gain $g2 = a + j b$ to produce the output $ui(n)$.

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The gain is updated at the beginning of the superframe, using the first two samples, denoted $y_i(n)$ and $y_i(n+1)$. In fact, the following matrix system is solved in the least squares sense.

$$\begin{vmatrix} y_{ir}(n) & -y_{ii}(n) \\ y_{ii}(n+1) & y_{ir}(n+1) \end{vmatrix} \begin{vmatrix} a \\ b \end{vmatrix} = \begin{vmatrix} 1 \\ 1 \end{vmatrix} \quad (7)$$

5 A preferred approximate implementation of the least squares algorithm is as follows

$$a = A / C \quad ; \quad b = B / C \quad (8)$$

where the quantities A, B and C are updated every superframe by

$$A(p+1) = (1-\epsilon) A(p) + \epsilon [y_{ir}(n+1) + y_{ii}(n)] \quad (9)$$

$$10 \quad B(p+1) = (1-\epsilon) B(p) + \epsilon [y_{ir}(n) - y_{ii}(n+1)]$$

$$C(p+1) = (1-\epsilon) C(p) + \epsilon [y_{ir}(n)y_{ir}(n+1) + y_{ii}(n)y_{ii}(n+1)]$$

The parameter ϵ is a small constant, for example $\epsilon = 10^{-2}$, p is the superframe index. The initial values can be $A(0) = 10^{-3}$, $B(0) = 0$ and $C(p)$ is kept no smaller than 10^{-2} .

15 Once the complex gain elements have been calculated, a real error signal is derived as follows.

$$e_{ip}(n) = 1 - [a y_{ir}(n) - b y_{ii}(n)] \quad (10)$$

$$e_{ip}(n+1) = 1 - [b y_{ir}(n+1) + a y_{ii}(n+1)]$$

The error signal is used for noise level estimation as described
20 below.

The fine equalizer 223 computes the following output

$$v_i(n+1) = u_i(n) + \sum_{k=-1}^1 h_k(n) u_i(n-k) \quad (11)$$

25 to be delivered to the data extraction module 230. The function of the fine equalizer is to complete the task of the two previous modules, in particular to remove the residual distortion. Its coefficients $h_k(n)$ generally take very small values and they can be updated at the superframe rate, using the same reference
30 signal as the phase equalizer 222. In addition, they can be updated during regular transmission, according to the data directed equalizer principle, using the error signal $e_i(n)$ provided by the data extractor 230 and the least mean squares (LMS) algorithm

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$$h_k(n+1) = h_k(n) + \delta e_i(n+1) u_i(n-k) \quad (12)$$

where δ , the adaptation step size, is a small value, for example $\delta = 10^{-3}$.

Turning back to FIG. 4, the capacity of a subchannel is
 5 determined by the « capacity+ bit assign » block 250. This block receives the error signal e_{ip} from the phase equalizer and the error signal e_i from the data extraction block 230. It computes the following two variables.

$$E1(p) = (1-\epsilon_1) E1(p-1) + \epsilon_1 [e_{ip}^2(n) + e_{ip}^2(n+1)] / 2 \quad (13)$$

$$10 \quad E2(n) = (1-\epsilon_2) E2(n-1) + \epsilon_2 [e_i^2(n)] \quad (14)$$

where the parameters ϵ_1 and ϵ_2 are small values like 10^{-2} and 10^{-3} respectively for example.

The quantity $E1(p)$ is computed every superframe and it is representative of the total distortion plus noise power present
 15 in the subchannel, before fine equalization. The quantity $E2(n)$ is computed at the rate 8 kHz and it is representative of the noise power in the subchannel. In normal operation, with the above equations (13) and (14), $E2(n)$ is smaller than $E1(p)$ and the difference depends on the improvement brought by the fine
 20 equalizer.

Based on the results of these calculations, a decision is made at the beginning of each hyperframe to keep or modify the number of bits assigned to each subchannel. Then, the corresponding information data, denoted « scdatae », are fed to the
 25 « synchro+data » block 150 of the emitter 100, for transmission to the distant terminal during the current hyperframe and to the data extraction block 230 in the receiver 200, for use during the next hyperframe. The determination of the number of bits N_b assigned to the subchannel is a two-step process. First, N_b is
 30 calculated, for example through successive comparisons to thresholds, as

$$N_b = \text{Int} [\frac{1}{2} \log_2 (1 / E1(p)) - 1] \quad ; \quad E1(p) < 0.25 \quad (15)$$

where $\text{Int}[x]$ stands for the integer part x . Then, $E2(n)$ is used
 35 to confirm the decision or improve it. For example, if $E2(n)$ is smaller than $E1(p)/4$, the number of bits may be increased by one.

The number of bits assigned to the subchannels is limited by the service data capacity. As pointed out earlier and shown

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in FIG. 3, the synchronization signal can transmit 14 bits of service data in a superframe with the numerical values given. If 3 bits are allotted to each subchannel, 4 subchannels can be handled per superframe and, if 240 subchannels are actually used, then, 60 superframes are sufficient to transmit the whole capacity information. The number of bits assigned to any subchannel is included in the range [0, 7].

The data extraction module 230 receives the signal $vi(n)$ from the subchannel equalizer 220 and performs a quantization operation on the real and imaginary parts alternatively, using the quantization scale associated with the number of bits assigned to the subchannel. The binary representation of the quantized value dir is fed to the parallel/serial converter 240 and the quantization error $ei(n)$ is sent back to the subchannel equalizer 220 to be used as per equation (12). The parallel/serial converter 240 produces the output data stream $d'(n)$.

The «synchro processing» block 270 is shown in more details in FIG. 6. It receives the synchronization subchannel signal x_{isr} and performs amplitude equalization through block 271, as described previously for the other subchannels. The signal obtained, $y_{is}(n)$ is fed to the «envelop detection» module 272 that computes the variable $v(n) = |y_{is}(n)|^2$. Then, the control signal $ca(4n)$ is generated by block 273 as explained above and according to equations (3) and (4).

The subchannel signal x_{isr} is also fed to an amplitude/phase equalizer 274 that produces a signal $u_{is}(n)$, from which the binary data at the rate 8 kHz are recovered, with the help of a data detector 275. In fact, the data detector just takes the sign of the real and imaginary parts of $u_{is}(n)$ alternatively. The binary sequence $bs(n)$ so obtained is fed to the «synchronization pattern and data extraction» block 276, that recognizes the superframe and hyperframe synchronization patterns and delivers the corresponding timing information denoted «timing 1/64» in the figures. The block also separates the bit assignment data, denoted «scdatar» and delivered to the OQAM modulator 120 of each subchannel and to the serial/parallel converter 110 in the emitter of the system.

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Industrial Applicability

An important feature of the system of the invention is that poor quality sections of the transmission channel frequency band can be exploited, through the combination of several subchannels.

5 In each superframe, the synchronization subchannel signal carries the bit assignment data for a group of 4 subchannels. If, for these 4 subchannels, the noise power estimations $E_{lj}(p)$ with $j=1, 2, 3$ and 4 , are all greater than 0.0625 , which means $N_b=0$, and if the following condition is satisfied

$$10 \quad \sum_{j=1}^4 (1 / E_{lj}(p)) > 16 \quad (16)$$

then, the same one-bit data signal is fed to these subchannels in the emitter and the corresponding phase equalizer outputs
15 $u_{i+j}(n)$ in the receiver are summed as follows

$$\text{sum}(n) = \sum_{j=1}^4 u_{i+j}(n) / E_{lj}(p) \quad (17)$$

and the input data are retrieved as the sign of the variable
20 $\text{sum}(n)$. With that technique, a one-bit data sequence is transmitted by 4 subchannels. Clearly, this is an example and similar combinations can be elaborated for other numbers of subchannels, like 2, 3, 8 or 16. The output $v_i(n)$ of the subchannel equalizer 220 may also be used.

25 Although the present invention has been described in terms of the presently preferred embodiment, it is to be understood that such disclosure is purely illustrative and is not to be interpreted as limiting. Consequently, without departing from the spirit and scope of the invention, various alterations,
30 modifications, and/or alternative applications of the invention will, no doubt, be suggested to those skilled in the art after having read the preceding disclosure. Accordingly, it is intended that the following claims be interpreted as encompassing all alterations, modifications, or alternative applications as fall
35 within the true spirit and scope of the invention.

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The Claims

What is claimed is:

1. A multicarrier digital transmission system comprising
5 an emitter (100) and a receiver (200):
 - a. the emitter (100) including:
 - i. means (110) for splitting an input data stream $d(n)$ into a number of substreams equal to a number of used subchannels;
 - 10 ii. means (120) for performing OQAM modulation on each substream and producing a set of N sequences x_i , each sequence being coupled to the input of a synthesis filter bank means (130) that produces a multicarrier output digital signal S_e ; and
 - 15 iii. means (150) for generating a synchronization and service data signal x_{is} in at least one subchannel of the system; and
 - b. the receiver (200) including:
 - i. analysis filter bank means (210) to produce from
20 an input signal S_r a set of sequences x_{ir} equal to the number of used subchannels, each sequence being coupled to an input of a subchannel equalizer means (220);
 - ii. data extraction means (230) to process equalizer
25 output and feed a parallel-to-serial converter means (240) that produces an output data stream $d'(n)$;
 - iii. means (270) for detecting a synchronization and service data signal;
 - iv. means (250) for estimating a noise level for
30 every subchannel and for deciding a number of bits to be assigned thereto,
- said system being characterized by, a subchannel equalizer (220) in the receiver (200) that includes a cascade of amplitude equalization means (221), phase and residual amplitude equaliza-
35 tion means (222) and fine equalization means (223).
2. An emitter and a receiver as defined in claim 1 wherein the signal transmitted by the synchronization subchannel (s)

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contains a superframe synchronization pattern and a hyperframe synchronization pattern.

3. An emitter as defined in claim 1, wherein the synchro-
5 nization and service data signal is transmitted by envelop modulation.

4. A receiver as defined in claim 1, wherein the envelop
of the synchronization and service data signal is used to produce
10 a signal to control the receiver sampling times and perform frame synchronization.

5. An emitter as defined in claim 1, wherein each
superframe the OQAM modulator (120) introduces a short fixed
15 sequence into the signal in each subchannel.

6. A subchannel equalizer (220) as defined in claim 1,
wherein the phase and residual amplitude equalizer (222) is
updated at a superframe rate, using a short fixed pattern
20 introduced by the emitter as its reference signal.

7. A subchannel equalizer (220) as defined in claim 1,
wherein the fine equalizer (223) is a decision directed equaliz-
er.
25

8. An emitter and a receiver as defined in claim 1,
wherein data for bit assignment in the subchannels are transmit-
ted each hyperframe, and the numbers of bits carried by each
subchannel are confirmed or modified each hyperframe.
30

9. An emitter and a receiver as defined in claim 1,
wherein the same input signal is fed to two or more subchannels
at the emitter and the outputs of the corresponding subchannel
equalizers (220) are combined to produce a signal from which the
35 data are extracted.

10. A combination of subchannel signals as defined in claim
9, wherein the combination is achieved by a weighted summation,

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the weighing coefficients being the inverses of the estimated total distortion powers, and the data are obtained by taking the sign of the weighted summation result.

- 5 11. An emitter and a receiver as defined in claim 1, wherein the coefficients in the filter banks (130) and (210) are such that the prototype filter response satisfies the first Nyquist criterion and the second Nyquist criterion.

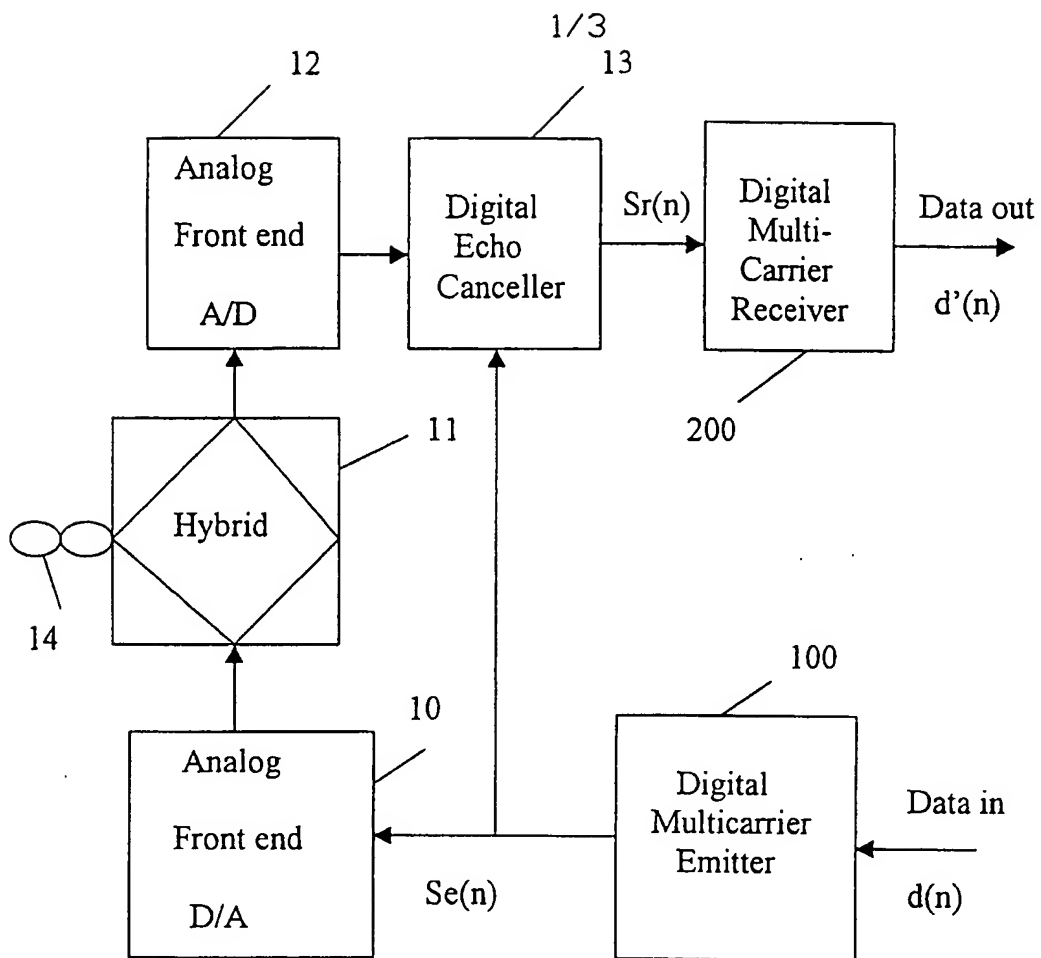


Fig.1. Multicarrier Transmission System

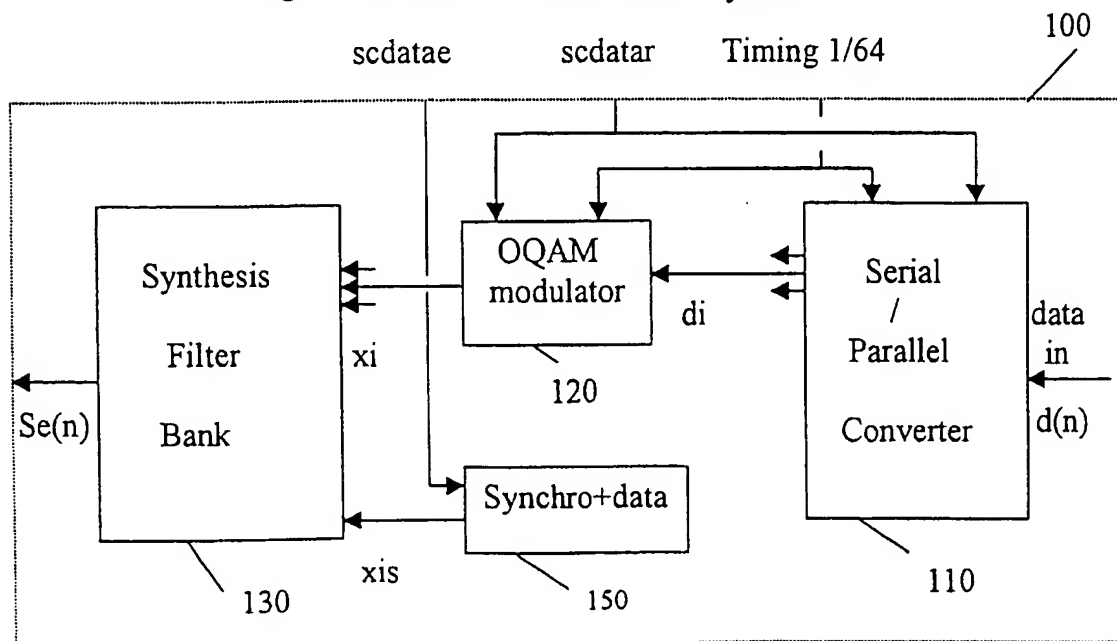


Fig.2. Digital Multicarrier Emitter

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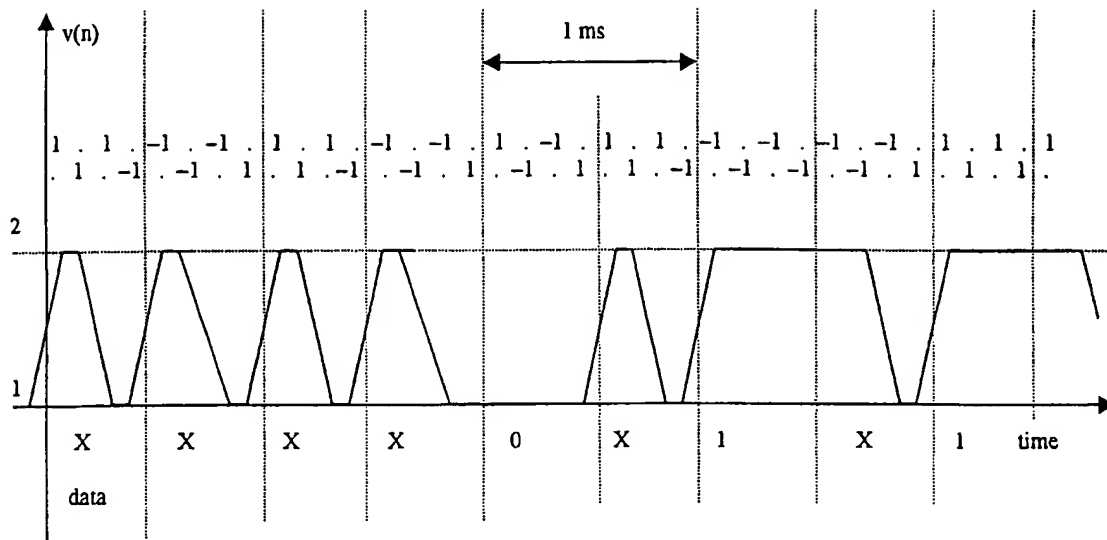


Fig.3. Synchronization subchannel signal

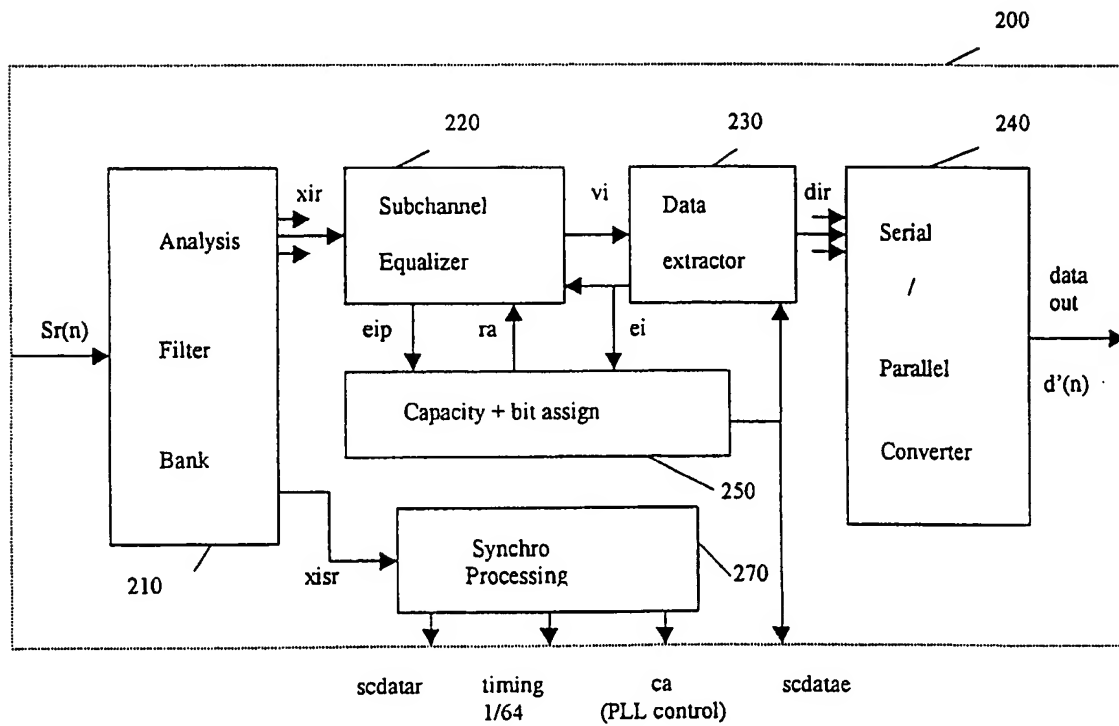


Fig.4. Digital Multicarrier Receiver

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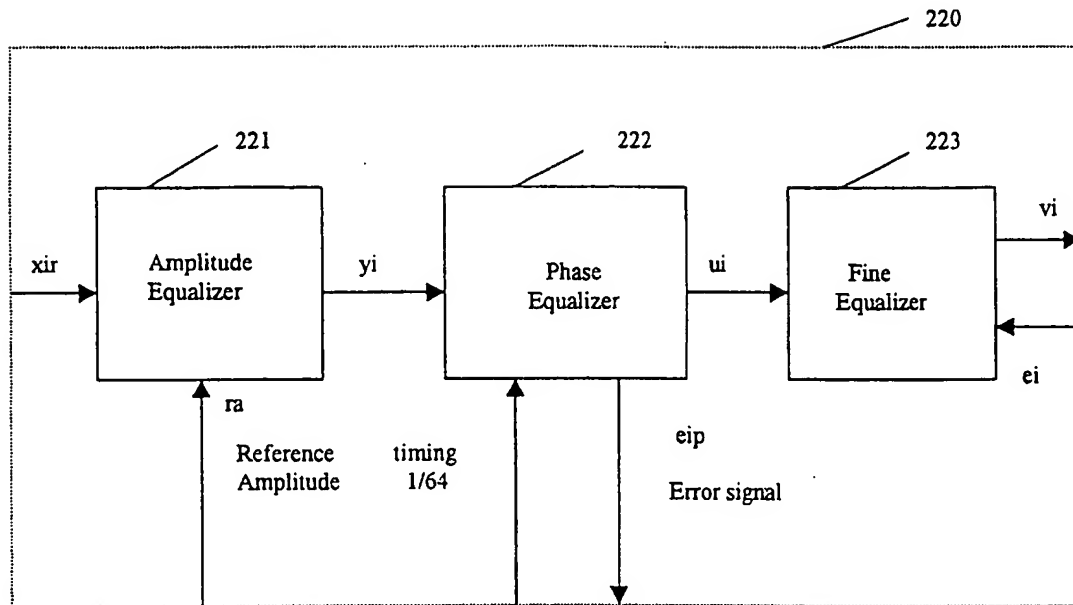


Fig.5. Subchannel Equalizer

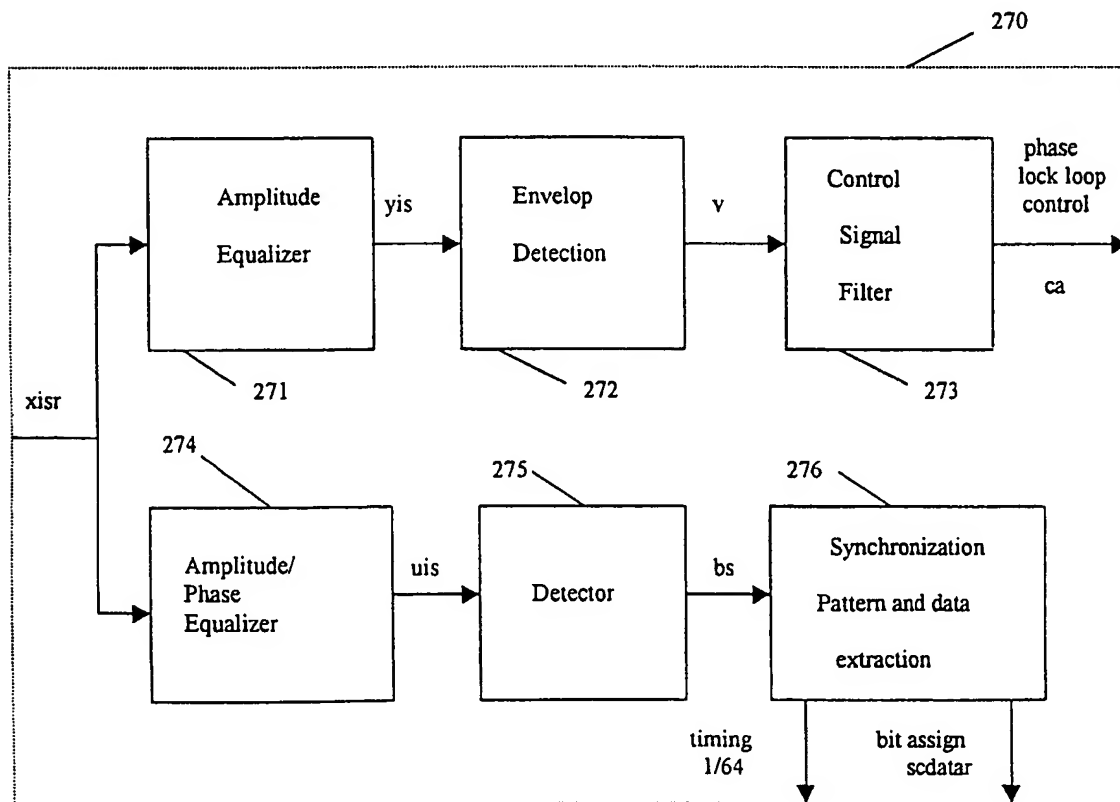


Fig.6. Processing of received synchronization channel

INTERNATIONAL SEARCH REPORT

International application No.
PCT/US00/42048

A. CLASSIFICATION OF SUBJECT MATTER IPC(7) : H04J 1/20; H04L 7/00, 27/01, 27/34 US CL : 375/230, 261, 298, 349, 350, 355; 370/483, 484, 497, 509 According to International Patent Classification (IPC) or to both national classification and IPC		
B. FIELDS SEARCHED Minimum documentation searched (classification system followed by classification symbols) U.S. : 375/229, 230, 232, 233, 260, 261, 298, 349, 350, 355; 370/480, 483, 484, 497, 509 Documentation searched other than minimum documentation to the extent that such documents are included in the fields searched NONE Electronic data base consulted during the international search (name of data base and, where practicable, search terms used) EAST search terms: synthesis filter, analysis filter, equalizer, multicarrier, subchannel, synchronization, OQAM, frames, amplitude, phase, fine		
C. DOCUMENTS CONSIDERED TO BE RELEVANT		
Category*	Citation of document, with indication, where appropriate, of the relevant passages	Relevant to claim No.
A, P	US 6,047,025 A (JOHNSON et al) 04 April 2000, see its entirety.	1-11
A	US 5,644,596 A (SIH) 01 July 1997, see its entirety.	1-11
A	US 4,853,802 A (KUKSON et al) 01 August 1989, see its entirety.	1-11
<input type="checkbox"/> Further documents are listed in the continuation of Box C. <input type="checkbox"/> See patent family annex.		
* Special categories of cited documents: "A" document defining the general state of the art which is not considered to be of particular relevance "E" earlier document published on or after the international filing date "L" document which may throw doubts on priority claim(s) or which is cited to establish the publication date of another citation or other special reason (as specified) "O" document referring to an oral disclosure, use, exhibition or other means "P" document published prior to the international filing date but later than the priority date claimed "T" later document published after the international filing date or priority date and not in conflict with the application but cited to understand the principle or theory underlying the invention "X" document of particular relevance; the claimed invention cannot be considered novel or cannot be considered to involve an inventive step when the document is taken alone "Y" document of particular relevance; the claimed invention cannot be considered to involve an inventive step when the document is combined with one or more other such documents, such combination being obvious to a person skilled in the art "&" document member of the same patent family		
Date of the actual completion of the international search 06 FEBRUARY 2001		Date of mailing of the international search report 03 APR 2001
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